

Analysing and simulating electronic devices as antennas

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Abstract – Electromagnetic compatibility is getting more and more interest as soon we are speaking about electronic devices. EMC must be planned, calculated, simulated, and measured to ensure that the device can work in the environment of other devices and does not disturb other devices by unwanted interference. In complex devices, simulation methods due to the large number of elements and complicated operations can be extremely costly and time consuming. We should consider how is it possible to reduce these costs, for example with simplifying our simulation terminology. This paper explains a general theory about using pre-measured EMC properties in simulation to find out how a complex system (containing many devices) will work out. This theory is about how different radiated electromagnetic waves have effects on other devices. Electromagnetic compatibility (EMC) standards have been developed to test and limit unintentional coupling to and from electronic devices (interference), but not developed to deal with more devices crowded in a smaller environment. If we handle the different devices as antennas, in the simulation environment we must not deal with their internal structure and operation (till we need information of the inside). This way simulation time can be drastically reduced.

Keywords – EMC simulation, devices as antennas, device simulation

I. INTRODUCTION

In all departments of electronic design and manufacturing, electromagnetic compatibility (EMC) is one of the most important factors. All of the devices need some kind of EMC in order to work properly. Some of them can be interfere with others easily, while others radiate lots of electromagnetic waves. Nowadays EMC is becoming more important than ever, because of the growing number of electronic devices, gadgets, smart devices we use.

The basic idea is if we know some radiation or immunity properties of the product, we could feed these

in simulation software. If we have the proper structural model of the product, we could simulate and analyse the properties and with the results, we can consider what changes must be made. An example is when a bigger structure, which contains metal parts, magnets, external wires and electronics, may be too complicated for complex simulations, but the different parts can be analysed as simple individual antennas. In this way, without simulating every working circumstances, some antenna-like characteristics can be achieved easily. This paper is a general overview of the problems and gives some basic ideas to solve them.

II. EMC PROBLEMS IN LONG TERMS

A common approach to achieve the required EMC levels starts when designing the device. This is the stage where most of the work can be done easily, without further costs. After design, prototypes can be manufactured and if required, EMC measurements are performed. If everything goes right, final manufacturing starts, and the product could get on the market. But what happens if after some time, we want this product to achieve higher EMC limits in special appliances, because of local laws, or other devices working next to it?

The costs of a new design and manufacturing process easily get high but improving the good working product can be worth it. Here comes a special idea about this improvement, if we know what we want to improve in the product, for example, in a frequency range it emits more EM waves than we want, we could analyse the structure directly as some antennason that specific range. In some cases, EMC measurements can declare the radiation characteristic, but it could be cost effective, if we could easily simulate this. Simulation is one side of determining the radiation properties of the product, but in function of internal structure and operation parameters, simulation time and computer requirements increase. Proper EMC chambers and test methods can't be avoided, but if we simulate only the “antenna properties” of the product, more information can be gained before proper measurements are made.

III. DEVICES AS ANTENNAS

Antennas can be made of a simple wire or complex metal structures, maybe some smaller block which act like a grid antenna. It is possible to look at our device as an antenna. Every electronic device contains metal parts, PCBs, wires, metal casings and so on. They are not optimized to work as antennas (in general conditions), but as unintentional antennas.

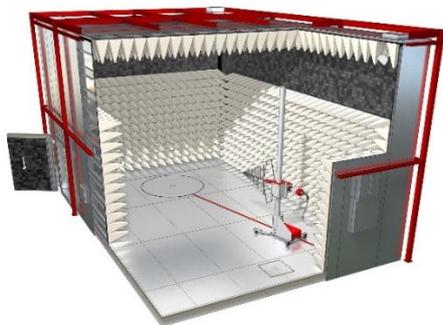
A. Gain and radiation pattern

Antennas are typically designed for specific usage with needed characteristics (like gain and pattern). This means they have a known frequency response, directivity, or pattern. On the other hand, simple devices are not intended for this type of use, so these parameters work on a larger scale. This means measurements on these unintentional antennas present some challenges compared to normal antenna tests. In some cases, for example commercial EMC tests, the entire 3D measurements must be done, while in automotive tests only a few directions must be measured. This is one reason why alternative methods to estimate the directivity, radiation pattern and other needed parameters are considered [1]. With estimation the number of tests can be decreased so the overall costs fall.

When determining the pattern of a receiving antenna by computer simulation, it is not necessary to perform a calculation for every possible angle of incidence. Instead, the radiation pattern of the antenna is determined by a single simulation, and the receiving pattern inferred by reciprocity. When determining the pattern of an antenna by measurement, the antenna may be either receiving or transmitting, whichever is more convenient. [2]

B. Measuring the device

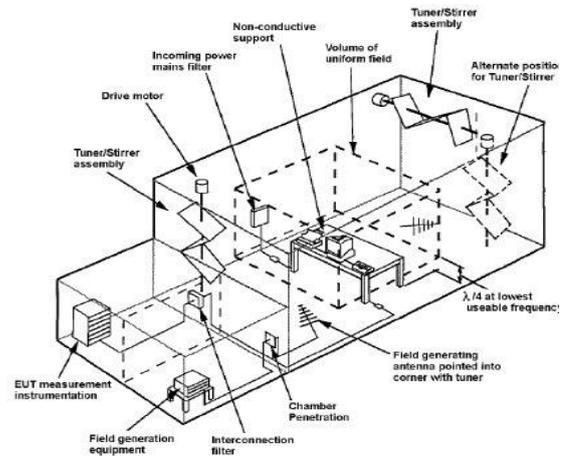
Nowadays the needed „3D” EMC measurements on every single device cost more, it can be worth the price by reducing the overall costs when designing a complex system. To measure the radiated power pattern (of any device) one method is to use a fully anechoic chamber (Figure 1.).



1. Fig. Semi Anechoic 3m EMC Chamber with traditional square design [3]

The receiving antenna must be equally far from source. The equipment under (EUT) test is mounted on a rotating table, while the receiving antenna mounted on vertical sliding base to move up and down. Each measurement is done in one position than rotating the EUT or lifting the antenna. From the measurements a ratio of the maximum to average power can be calculated for each planar cut.

Another method uses a reverberation chamber (Figure 2.).



2. Fig. The reverberation chamber as described in IEC-61000-4-21 [4]

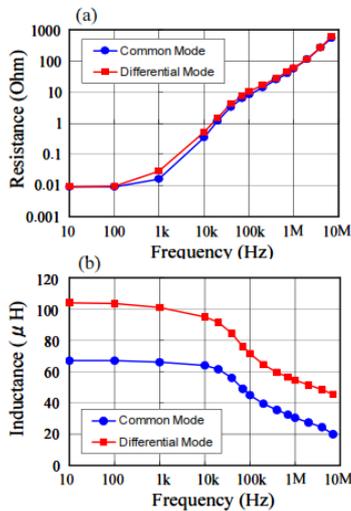
This type of chamber is usually used for immunity testing but can also provide an efficient method for radiated emission measurements. Results of these measurements yield the total radiated power, not directivity properties. Using this method, further simulation methods will lack of possibility to use shielding or design other orientation based on radiation data. In some cases, it is possible that these results may provide enough information to avoid later EMC problems.

IV. SIMULATING EMC PROPERTIES

Without the required EMC measuring technology, electromagnetic simulation of the device can result in antenna like properties. There are several types of simulating software on the market. Numerical simulations can provide full EMC properties, but to inspect a bigger complex system, it needs lots of computing time. Even though precise and complex simulation is not the most cost-effective solution, on a lower, individual parts level can be worth it. Ideally, however, it is better to minimize the measurement-based revision by taking preventive measures in the design stage. Numerical simulations are useful for both purposes, i.e. not only to realize observed phenomena and find effective countermeasures early, but

also to predict phenomena without measurement in the design stage.

Modelling a BLDC motor especially for EMC simulation is presented in [5]. BLDC motors are a good point in the EMC topic, because they get more and more popular, but also due to their working conditions, can suffer from lots of electromagnetic problems. The sum of instantaneous voltage of three-phase windings of a motor (also 2-phase windings), or common-mode voltage, is not zero in this system. Furthermore, the switching frequency is increasing with the development of switching devices such as IGBTs. These facts cause high-frequency leakage current, which leads to EMI/EMC issues. The common-mode voltage also provokes a shaft voltage, which causes a bearing current. The bearing current damages a bearing and makes its lifetime shorter. In addition, high-frequency switching causes overvoltage and turn-to-turn voltage stress in stator windings, which affects its insulation seriously. It is possible that modern simulation software on a fast-enough computer can simulate the most required parameters, but in [5] the entire simulation process is taken in different parts to increase efficiency. Models are made for electromagnetic field analysis, independently calculated capacitance by static electric field analysis and inductance with resistance by magnetic field analysis.

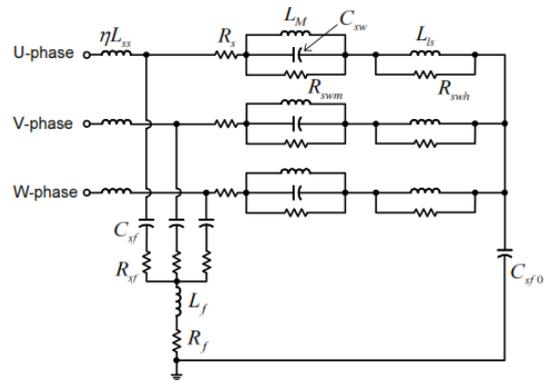


3. Fig. Calculated (a) resistance and (b) inductance of stator windings per phase for common mode and differential mode. [5]

The analysis with the 3-D model, i.e. a motor with laminated iron core, the effect of eddy current becomes significant only above 1 kHz. Furthermore, magnetic flux is not completely pushed out of the iron core even at 1 MHz, and thus the inductance remains about half of the value for low frequencies. The resistance in case of laminated iron core (3-D analysis) is larger than that in case of bulk iron core (2-D analysis) above 20 kHz. This is because the surface area where eddy current flows is

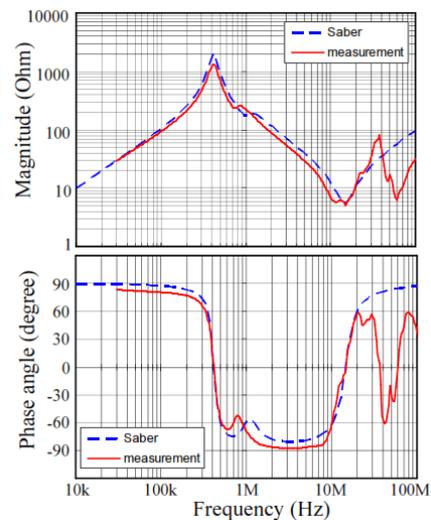
larger and thus the total power loss is larger in laminated iron core for such high frequencies. In this way, with 2-D mesh data, it is likely to overestimate the shielding effect of eddy current in laminated iron core. Therefore, we should use 3-D mesh data to calculate inductance and resistance of stator windings accurately. [5]

This means that precise simulation requires different approaches, there is no straight-forward solution for it. With the different simulation results it is possible to construct a high-frequency motor equivalent circuit (Figure 4. shows an example for a BLDC motor).



4. Fig. Equivalent circuit of a three-phase Y-connected BLDC motor: [6]

It means that 2D and 3D simulation software is not longer needed, because we only need the results of previous mentioned simulations. The equivalent circuit contains the data of resistance, inductance and capacitance of the stator windings, so after some "basic" calculation we can achieve a frequency characteristic of the motor impedance (Figure 5.).



5. Fig. Frequency characteristic of motor impedance for differential mode (magnitude and phase angle) by the equivalent circuit [5]

Magnitude and phase angle both can be calculated, so the whole process can result in the required antenna parameters.

These numerical simulations are not relevant in fine tuning a real motor, because there are more phenomena (such as hysteresis, permeability, magnetic saturation) and lack of factors like manufacturing imperfection, temperature, aging. But it is possible to use the results further for our needs.

V. ESTIMATION OF DIRECTIVITY

If measuring the device in the mentioned EMC chamber conditions and simulating the EMC properties of the device, estimating them can be a good alternative solution to get the required parameters. This section is based on [7], [8], where a theory of estimating not all antenna parameters, but the directivity. Directivity of an antenna (or device as antenna) is the evaluation of far-field form of the spherical mode expansion of the emitter. The assumption is the expansion coefficients are independent random variables. Equation (1) shows the general form for the far-field pattern (in 3D spherical coordinate system expressed with polar coordinates).

$$\bar{E}(r, \theta, \vartheta) = k\sqrt{\eta} \frac{1}{\sqrt{4\pi}} \frac{e^{jkr}}{kr} \sum_{smn} Q_{smn}^{(3)} \overline{K_{smn}}(\theta, \vartheta) \quad (1)$$

where the spherical coordinate system is defined as usual, η is the free space wave impedance,

$$\sum_{smn} = \sum_{s=1}^2 \sum_{n=1}^N \sum_{m=-n}^n N \approx ka \quad (2)$$

where a is the radius of the minimum sphere enclosing the emitter (it is assumed the spherical coordinate system is centered in this sphere), ka is called the electrical size, $Q_{smn}^{(3)}$ are the wave coefficients, and $\overline{K_{smn}}(\theta, \vartheta)$ are the far-field large argument, forms of the dimensionless power-normalized spherical wave functions.[9] This convention yields the expression (3).

$$P_{rad} = \frac{1}{2} \sum_{smn} |Q_{smn}^{(3)}|^2 \quad (3)$$

Expression (3) shows the total radiated power (P_{rad}) from the emitter. In general, the summation over n goes to infinity; however, spherical wave functions with indices $n > ka$ are cut off and will not contribute in the far-field and, because of this, the series can be truncated.

$$N_m = 2 \sum_{n=1}^N (2n + 1) = 2(N^2 + 2N) \quad (4)$$

where Nm is the total number of modes. Each coefficient has an independent real and imaginary part. With this expression an upper bound can be found. Directivity is the ration of radiated power (at a given

angle) and distance to the total radiated power divided by the total solid angle. The Cauchy-Schwartz inequality yields a sum over the number of modes (Nm), that is reduced by a factor of two. The result expression below once (ka) is substituted for N :

$$D_{max} \approx \begin{cases} 3, ka \leq 1 \\ (ka)^2 + 2ka, ka > 1 \end{cases} \quad (5)$$

The only problem here is D_{max} is an overestimation of the directivity of unwanted antennas. A better estimation can be derived by assuming that the spherical-wave coefficients are independent random variables.

For unintentional emitters, the mean of co- and cross-polarized terms will be equal, so the mean value of D is 1.

$$\overline{D_{co}} = \overline{D_{cross}} = 1/2 \quad (6)$$

The field components of expression (1) is the following:

$$|\overline{E_{\theta}}(r, \theta, \vartheta)|^2 = \frac{\eta}{4\pi r^2} \left| \sum_{smn} Q_{smn}^{(3)} \overline{K_{smn}}(\theta, \vartheta) \cdot \bar{\alpha}_{\theta} \right|^2 \quad (7)$$

$$|\overline{E_{\vartheta}}(r, \theta, \vartheta)|^2 = \frac{\eta}{4\pi r^2} \left| \sum_{smn} Q_{smn}^{(3)} \overline{K_{smn}}(\theta, \vartheta) \cdot \bar{\alpha}_{\vartheta} \right|^2 \quad (8)$$

As mentioned earlier that the real and imaginary parts of $Q_{smn}^{(3)}$ are independent and Gaussian distributed with zero mean. The directivities D_{co} and D_{cross} is similarly distributed. The expected value for the maximum over N_s samples of a χ^2 with two degrees of freedom distribution is:

$$\overline{D_{co,max}} = \overline{D_{co}} \sum_{n=1}^{N_s} \frac{1}{n} \quad (9)$$

This summation can be approximated and substituting the expected value of D_{co} from (6) yields expression (10).

$$\overline{D_{co,max}} \approx \frac{1}{2} \left[0,577 + \ln(N_s) + \frac{1}{2N_s} \right] \quad (10)$$

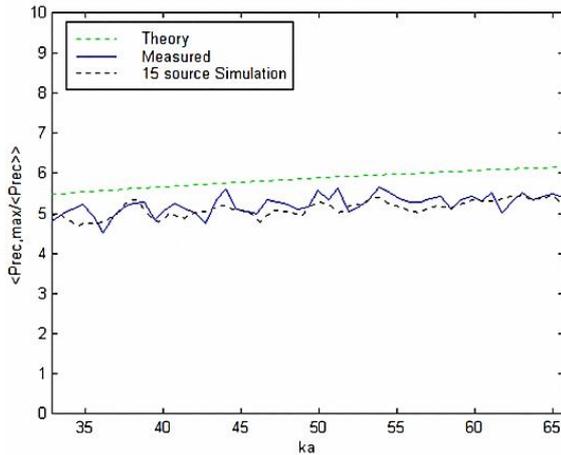
If $ka > 1$, $N_s = 2N_m$ and $N = ka$ expression (10) results in (4). For $ka = 1$ ($N_s = 12$), (10) yields $\overline{D_{co,max}} \approx 1,55$.

A physical interpretation of $N_s = 12$ for $ka \leq 1$ is that the real and imaginary parts of six dipole moments (three electric and three magnetic) yield 12 independent source contributions. The directivity estimate is also very near the directivity of a single short dipole ($D = 1.5$). Thus, using 1.55 for electrically small emitters in (10) results in a continuous function and should give good estimates for directivity:

$$\overline{D_{max}} \approx \begin{cases} 1,55, k \leq 1 \\ \frac{1}{2} \left[0,577 + \ln(4(ka)^2 + 8ka) + \frac{1}{8(ka)^2 + 16ka} \right], ka > 1 \end{cases} \quad (11)$$

The main difference between the intentional emitter upper bound given by (5) and the unintentional emitter expected value given by (11) is that the upper bound increases rapidly as the square of the electrical size ka , while the expected value increases only as the natural logarithm (\ln) of electrical size ka .

The estimated, measured and simulated total radiated power ratio for an example EUT are compared in [1].



6. Fig. The estimated (theory), measured, and simulated ratio for an example EUT [1]

Figure 6. shows that the result of measurements and simulation is pretty much close together, but the theoretical estimation is neither too bad. This means that estimation can be used instead of measurement and simulation, but if higher precision is needed, they cannot be ignored.

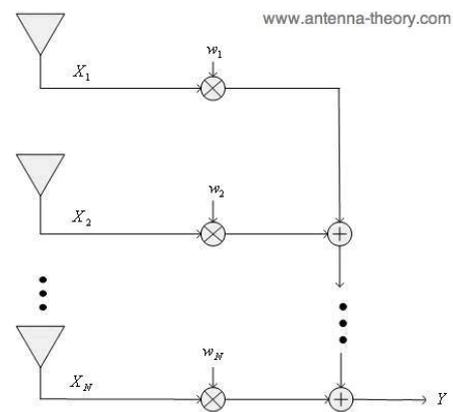
The theory also shows that in earlier stages only estimation can be enough to determine the overall EMC performance. This can further reduce costs, because we do not need actual measurements or time-consuming simulation processes to get antenna like properties.

On the other hand a large and complex device containing many different parts is usually made of such individual components that their EMC properties are measured by the manufacturer (for example in automotive industry, every electronic component should pass EMC restrictions before building into the actual vehicle), so this type of estimation or simulation process can be skipped.

VI. ANTENNA ARRAYS

At his point we should have all the parameters to handle our individual devices as antennas. Measurements, simulations, and estimations must give enough information about the product. When assembling the final, complex device made of the individual devices we can treat it like an antenna array. A classical antenna array (often called a 'phased array') is a set of 2 or more

antennas. The signals from the antennas are combined or processed to achieve improved performance over that of a single antenna. These types of antennas can be used to increase overall gain, maximize the signal to interference plus noise ratio, direct the array so that it is most sensitive in a direction, cancel out interference and so on [10]. These applications (some of them with reciprocity) are also the basics of decreasing overall EMC performance of a complex system. In a phased array it is not so hard to add together the different antennas, because they are usually consisting of similar ones and made symmetrically. There is a weighting of the different antennas (Figure 7.).[2]



7. Fig. Weighting and summing of signals from the antennas to form the output in a Phased Array [10]

Classical antenna arrays are made for specific reasons, but in our case, the different devices according to their operation, orientation, and distance from each other act like transmitters, but also receivers. If we choose one operation where we handle all of them as receivers, we can calculate the EMI properties. Next to the weighting we need to include distance and directivity factors to get accurate results. We can calculate the overall power of radiated electromagnetic waves if we handle all of them like transmitters. And finally if we want a mixed operation calculation, because we know that some of the individual devices work more like transmitters (emits more EM waves than they are immune to) and some of them work more like receivers (they are sensitive to EM waves but does not radiate so much) we need calculate them one by one. This method is like superposition in electrotechnics but with antennas.

Weighting, antenna factors, distances, directivity properties must stay, but they can be "switched off" one-by-one and in a round calculate the effect on all the others, then finally sum-up the results of each round. In each iteration it is possible to inspect the effect of only one device on the others or choosing several iterations to select a group of devices. It yields a similar result if we take the complex system, put it in an EMC chamber and

measuring. After one complete measurement we switch off some devices, or just leave a little group of devices and measuring again the EMC. The cost of only calculations and measurements cannot be compared.

VII. POSSIBLE ERRORS

This general theory is based on devices as antennas so one thing must be mentioned is conducted EMC. It is acceptable to measure the connecting wires, but real-life application may use cables different in length, diameter, shielding properties, etc. Although we know the radiation pattern and radiated immunity of the product, but if we want proper results of the simulation, we must inspect the connecting wires also. It is not the most important in all applications but for example in automotive industry where lots of wires inside a metal body crowded with electronics, the problem should be solved.

Another possible factor is the passive, shielding like parts in the complex system. Mountings, covers, design elements made from metal can easily distort the results. If we take them in count like the "active" devices, the risk of error decreases, but this procedure highly enlarges the number of devices.

The less precise properties we use, the less precise results we get. If EMC measurements or proper simulations are not available, we can estimate the performance of the device but in the more cases we calculate with estimations, the results may not meet our expectations in precision.

VIII. CONCLUSIONS AND OUTLOOK

This paper provided a theory of handling devices as antennas to easily calculate EMC properties if more devices are used in a closer area. This scenario appears easily in electrical boxes, vehicles or in our house because we use more and more electronic devices. To achieve results, we need antenna like properties of the device, like overall gain, frequency chart, directivity, and other factors. These can be gained from measurements in proper EMC chamber, 3D simulations and calculations or estimations. With these we must calculate the final performance of this antenna array with different methods depend on what performance parameter we need.

Further research on this theory must be done because the whole process (in ideal circumstances) can easily cut-off costs in designing and EMC testing. Also, to prove the concept example systems should be build up to try the different approaches.

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